Power System Analysis for Nonsinusoidal Steady State Studies Based on Wavelets

A. Ketabi¹  M. Khoshkholgh²

¹ Assistant Professor, Electrical Engineering department, University of Kashan, Kashan, Iran
Email: aketabi@kashanu.ac.ir

² PhD Student, Electrical Engineering department, University of Kashan, Kashan, Iran
Email: m.khoshkholgh@gmail.com

Abstract:
In this paper power system model is represented in a new domain that relates to Multi-Resolution Analysis (MRA) space. By developing mathematical model of elements in this space using Galerkin method, a new alternative method for power system simulation in nonsinusoidal and periodic conditions is developed. The mathematical formulation and characteristics of new proposed space is expressed. Also the relation between this domain and spectral analysis is presented. Transmission line and switching devices modeling in the proposed domain is investigated. To consider frequency dependency of line parameters and to obtain harmonics information, the relationship between this dependency and the new suggested domain is discussed. Then the new algorithm is presented and demonstrated for two case studies.

Keywords: Power system model, Multiresolution Analysis, Galerkin method, Spectral analysis, Distributed transmission line.

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Corresponding author: A. Ketabi
Address of corresponding author: Department of Electrical Engineering, Kashan University, Kashan, Iran
1. Introduction

New power systems include nonlinear, switching and frequency dependent elements. For example overhead lines, underground cables and impedances of transformers are frequency dependent elements due to skin effect and existence of harmonics that produced with switching devices. To investigate and estimate the harmonic content and propagation in a network with such elements, an algorithm for calculating the periodic steady state solution is required. Different algorithms to this end have been developed by many researchers. These algorithms are classified in terms of their formulation methodologies, into three categories: harmonic domain methods [1, 2], time domain methods [3, 4] and hybrid methods [5, 6]. In the harmonic domain method all network elements are expressed in the harmonic domain. Noninteger harmonics considered in harmonic sources is however an important concern in this method. Also, when one deals with the devices such as switching and nonlinear elements, the number of considered harmonics and coupling between them can make difficulties in numerical solutions [1].

In time domain method the nonlinearity and switching are modeled with ease, but frequency dependency of elements is a complicated concern. In the other hand, as in harmonic studies for the case of the steady state solution, the transient response of system must be eliminated by adjusting the initial conditions [4].

In recent years wavelet transform is used in power engineering. Despite the major abilities of this tool, its application is limited to signal processing for power quality usage. The base of this transform refers to MRA space, and this space has unique features. By using differential equations theory, the power system such as Fourier space can be represented in this space. New methods for power system analysis in MRA space are introduced by other authors in [7, 8]. The speeds of solution described in these papers make them inefficient for numerical simulation and are hence impractical for a real power system with relevant large dimension.

In this paper MRA space is used for power system simulation in nonsinusoidal and periodic conditions. Wavelet-Galerkin method guarantees the validation of this study from the mathematical point of view [13]. In MRA space a new space suitable for numerical analysis of power system is used. Investigating the features of the new space shows close similarity between it and the harmonic domain.

The paper is organized as follows: In section II a brief description of mathematical theory is presented. In section III the mathematical formulation is expressed. In this section the representation of power system in the new suggested domain is described. In section IV the relationship between this domain and spectral analysis is illustrated. In section VI distributed transmission line modeling is investigated. Two case studies in sections V and VII are simulated in the new domain and the results of these simulations are compared with a time domain simulation.

2. Mathematical Theory

2.1. Galerkin Method

The Galerkin method is one of the most reliable methods for finding numerical solution to differential equations [13]. Its simplicities make it perfect for many applications. The Galerkin approach is based on finding a functional basis for the solution space of the equation, then projecting the solution on it, and minimizing the residual with respect to the functional basis. Standard polynomial basis or trigonometric basis is used for Galerkin method. However wavelets used to describe MRA space often offers additional improvement to the above by providing both time and frequency localization. This means not only all dilations from an unconditional orthonormal bases of \( L^2(\mathbb{R}) \) are translated but scaling functions of all dilations for such bases for \( V_j \subset L^2(\mathbb{R}) \) are also translated.

2.2. Multiresolution Analysis

In this section the orthonormal basis of compactly supported wavelets is reviewed briefly. The orthonormal basis of compactly supported wavelets of \( L^2(\mathbb{R}) \) is formed by the dilation and translation of single function \( \psi(x) \) [10]:

\[
\psi(x) = 2^{-j/2} \psi(2^{-j} x - k)
\]

Where \( j, k \in \mathbb{Z}, \) the function \( \psi(x) \) has a companion: the scaling function \( \phi(x), \) and these functions satisfy the following relations:

\[
\phi(x) = \sqrt{2} \sum_{k=0}^{2^j-1} h_k \phi(2x - k)
\]

\[
\psi(x) = \sqrt{2} \sum_{k=0}^{2^j-1} g_k \phi(2x - k)
\]

The number \( J \) of coefficients in (2) and (3) is related to the number of vanishing moments \( M, \) and for the wavelets here \( J = M. \) The wavelet basis induces a MRA on \( L^2(\mathbb{R}), \) i.e. the decomposition of Hilbert space into a chain of closed spaces:

\[
L \subset V_1 \subset V_2 \subset V_3 \subset V_4 \subset V_5 \subset V_6 \subset V_7 \subset \cdots \subset L
\]

Such that:

\[
\bigcup_{j \in \mathbb{Z}} V_j = L^2(\mathbb{R})
\]

By defining \( W_j \) as an orthonormal complement of \( V_j \) in
2.3. Wavelet-Galerkin Solution of a Periodic Problem

To have a view of solution method in the MRA space, consider the following problem:

\[ L(u) = f, \quad f(0) = f(T) \]  \hspace{1cm} (8)

Where \( L \) is the differentiation operator. Suppose \( u \) and \( f \) have projections to MRA space such as below:

\[ u_{j+1}(x) = \sum_{k=0}^{2^{-j-1}} v_k^u \varphi_{j,k}(x) + \sum_{k=0}^{2^{-j-1}} w_k^u \psi_{j,k}(x) \]  \hspace{1cm} (9)

\[ f_{j+1}(x) = \sum_{k=0}^{2^{-j-1}} v_k^f \varphi_{j,k}(x) + \sum_{k=0}^{2^{-j-1}} w_k^f \psi_{j,k}(x) \]  \hspace{1cm} (10)

Using (9) and (10), equation (8) can be written as follow:

\[
\sum_{k=0}^{2^{-j-1}} v_k^u L(\varphi_{j,k}(x)) + \sum_{k=0}^{2^{-j-1}} w_k^u L(\psi_{j,k}(x)) = \sum_{k=0}^{2^{-j-1}} v_k^f L(\varphi_{j,k}(x)) + \sum_{k=0}^{2^{-j-1}} w_k^f L(\psi_{j,k}(x))
\]  \hspace{1cm} (11)

By taking an inner product with \( \varphi \) and \( \psi \), in the MRA space the equation (8) can be written in this matrix form [15]:

\[ S_j u = f \]  \hspace{1cm} (12)

The decomposition \( V_{j+1} = V_j \oplus W_j \) allows the operator \( S_j \) to be spitted into four pieces (\( W_j \) is called the wavelet space and the detail or fine-scale component of \( V_{j+1} \)) which can be written as follows:

\[
\begin{pmatrix}
A_{sj} & B_{sj} \\
C_{sj} & T_{sj}
\end{pmatrix}
\begin{pmatrix}
d_{sj} \\
s_{sj}
\end{pmatrix} =
\begin{pmatrix}
d_{sj} \\
s_{sj}
\end{pmatrix}
\]  \hspace{1cm} (13)

Where:

\[ A_{sj} : W_j \rightarrow W_j, \quad B_{sj} : V_j \rightarrow W_j \]
\[ C_{sj} : W_j \rightarrow V_j, \quad T_{sj} : V_j \rightarrow V_j \]  \hspace{1cm} (14)

And \( d_{sj}, s_{sj} \in W_j \), \( s_{sj}, s_{sf} \in V_j \) are the \( L^2 \)-orthonormal projections of \( x \) and \( f \) onto \( W_j \) and \( V_j \) spaces. The projection \( s_{sj} \) is the coarse-scale component of the solution \( x \), and \( d_{sj} \) is the fine-scale component. To solve (12):

\[ R_{sj} = T_{sj} - C_{sj} A_{sj}^{-1} B_{sj} \]  \hspace{1cm} (15)

\[ s_s = R_{sj}^{-1}(s_j - C_{sj} A_{sj}^{-1} d_j) \]  \hspace{1cm} (16)

\[ d_s = A_{sj}^{-1}(d_s - B_{sj} s_s) \]  \hspace{1cm} (17)

At this stage \( T_{sj} \) is selected and investigated. As the problem described above is periodic and supposing that the operator \( L \) is equal to \( d^n / dx^n \), the general form of \( T_{sj} \) is:

\[
T_{sj} = \begin{pmatrix}
\Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} \\
M & M & L & M & M & M \\
M & M & L & M & M & M \\
0 & 0 & L & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} \\
0 & 0 & L & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)} & \Omega_{s_j}^{(m)}
\end{pmatrix}
\]  \hspace{1cm} (18)

The general forms of the other pieces of \( S_j \) are also similar to \( T_{sj} \). For a circulant matrix [16] such as \( T_{sj} \), the eigenvalues \( \lambda_u \) are:

\[ \lambda_u = \sum_{i=0}^{N-1} \Omega_{s_j}^{(m)} \exp(-2\pi iat k/n), \quad a = 0, 1, L, n-1 \]  \hspace{1cm} (19)

And the corresponding orthonormal eigenvectors \( v_u \) are:

\[ (v_u)_k = \left( \frac{(-1)^n}{\sqrt{n}} \right) \exp(-2\pi iatk/n), \quad k = 0, 1, L, n-1 \]  \hspace{1cm} (20)

These relations lead to provision of quasi-diagonal form of represented operators in MRA space without using conventional methods in a lower time. Using diagonal form offers several advantages that are explained in the next parts. Using (19) and (20), (13) can be rewritten as:

\[
\begin{pmatrix}
A_{sj} & B_{sj} \\
C_{sj} & T_{sj}
\end{pmatrix}
\begin{pmatrix}
d_{sj} \\
s_{sj}
\end{pmatrix} =
\begin{pmatrix}
d_{sj} \\
s_{sj}
\end{pmatrix}
\]  \hspace{1cm} (21)

Where in (21):

\[ \hat{d}_{sj} = \Gamma^{-1} d_{sj}, \hat{s}_{sj} = \Gamma^{-1} s_{sj} \]  \hspace{1cm} (22)

\[ \hat{d}_{sj} = \Gamma^{-1} d_{sj}, \hat{s}_{sj} = \Gamma^{-1} s_{sj} \]  \hspace{1cm} (23)

In these equations \( \Gamma \) is the modal matrix. The columns of \( \Gamma \) are calculated using (20). \( A_{sj}, B_{sj}, C_{sj} \) and \( T_{sj} \) are diagonal matrices and their elements calculated by (19).

So to calculate \( \hat{d}_{s_{sj}}, \hat{s}_{s_{sj}} \) (the \( i \)th values of \( \hat{d}_{sj} \) and \( \hat{s}_{sj} \)), the following equation must be solved:

\[
\begin{pmatrix}
a_{fj} & b_{fj} \\
c_{fj} & d_{fj}
\end{pmatrix}
\begin{pmatrix}
\hat{d}_{s_{sj}} \\
\hat{s}_{s_{sj}}
\end{pmatrix} =
\begin{pmatrix}
\hat{d}_{fj} \\
\hat{s}_{fj}
\end{pmatrix}
\]  \hspace{1cm} (24)
The volume of calculations is decreases using the above technique significantly. In the other word instead of calculating the inverse of matrices with $N/2 \times N/2$ dimensions in (12), (24) is used for $N/2$ iterations. For problems with small dimensions this method seems not to be beneficial, however as shown in the following sections in this article this approach could be very useful for solving differential equations of large power systems, as in such systems the dimension of $S_j$ in (12) is obtained by the multiplication of the system dimension and the number of considered samples ($N$). Multiplications with $\Gamma$ introduces a new mapping to a new domain.

3. Power System Representation in The New Domain

3.1. Linear Elements Representation

The aim of this part is to obtain the expression for linear elements using mathematical operator representation in the new suggested domain. In this work modeling in the MRA space has been carried out on the same basis as suggested by other researchers [7, 8]. This mathematical expression should be a complete and meaningful one for power system studies in nonsinusoidal and periodic conditions. Major linear elements for power system, i.e. Resistors, Inductors and Capacitors are discussed briefly underneath:

3.1.1. Resistor

The relationship between voltage and current of a resistor in the time domain is:

$$v(t) = ri(t)$$

(25)

(25) in the new domain (as explained in section 2) is:

$$\begin{bmatrix} V_{dj} \\ V_{sj} \end{bmatrix} = \Gamma \begin{bmatrix} U & 0 \\ 0 & U \end{bmatrix} \begin{bmatrix} I_{dj} \\ I_{sj} \end{bmatrix}$$

(26)

In (26), $U$ is a unit matrix with dimensions of $N/2^{(j_{\text{max}}-j+1)}$.

3.1.2. Inductor

The relationship between voltage and current of an inductor is:

$$v(t) = \frac{di(t)}{dt}$$

(27)

So $N$ point discretization of (27) leads to:

$$V = \Gamma D_T \hat{I}$$

(28)

In (28) $D_T$ is the discretized form of derivative operator and $\hat{I}$ is a scalar. As the purpose is to obtain periodic solution, $D_T$ is a circulant matrix. In the MRA space (28) can be written as:

$$\begin{bmatrix} V_{dj} \\ V_{sj} \end{bmatrix} = \Gamma D_T \begin{bmatrix} I_{dj} \\ I_{sj} \end{bmatrix}$$

(29)

Where:

$$WD_T = \begin{bmatrix} HD_T H & 0 \\ LD_T H & LD_T L \end{bmatrix} = \begin{bmatrix} A_{sj} & B_{sj} \\ C_{sj} & T_{sj} \end{bmatrix}$$

(30)

To transfer (29) from highest level (finest scale) to next lower level (coarser scale) and respectively in a hierarchical form to other levels (scales) of MRA space, $D_T$ is substituted with $LD_T L$ of the higher resolution level. Of course in each subsequent level the dimensions of matrices will be different from previous ones and its magnitude is divided by 2. The sub-matrices of $WD_T$ have a circulant form and this feature is specific to all of orders of derivative operator in MRA space. Also the $\Gamma$ matrix and eigenvectors are the same for all orders in each level of MRA space. Rewriting (30) using (19) and (20) leads to obtain a quasi-diagonal form such as follow:

$$\begin{bmatrix} V_{dj} \\ V_{sj} \end{bmatrix} = \Gamma \hat{WD_T} \begin{bmatrix} \hat{I}_{dj} \\ \hat{I}_{sj} \end{bmatrix}$$

(31)

$$WD_T = \begin{bmatrix} HH & HL \\ LH & LL \end{bmatrix}$$

(31)

Where $\hat{WD_T}$ defines the impedance of inductor in the new suggested domain. There are four sub-matrices for impedance definition of inductor, the first sub-matrix ($\Gamma \hat{HH}$ deals with $W_j \rightarrow W_j$) belongs to high frequency part of level $j$. Also the fourth sub-matrix ($\Gamma \hat{LL}$ relates to $V_j \rightarrow V_j$) represents the impedance in low frequency part. The Fig. 1 shows the impedance of an inductor in the new domain for three scales.

By increasing the number of considered scales the accuracy of represented impedance in the new suggested domain is increased. The number of levels (scales) depends on the order of wavelet filter and the number of samples taken. In power system analysis, the frequency band is limited. Therefore, an acceptable accuracy can be reached by considering 3 or 4 levels. Between high frequency part and low frequency part there is a coupling that is represented by $\Gamma \hat{HL}$ and $\Gamma \hat{IH}$, however these parts are not as important as the cited parts ($\Gamma \hat{HH}$ and $\Gamma \hat{LL}$).
3.1.3. Capacitor

There is a time domain relationship between the voltage and current of a capacitor which can be discussed as follows:

\[ v(t) = \frac{1}{c} \int i(t) \, dt \]  
(32)

In discrete form (32) is written as below:

\[ V_i = \frac{1}{c}[D_T]^{-1} \vec{L} \]  
(33)

\[ D_T^{-1} \] is the discrete form of integral operator in periodic conditions. The transferred form of \( D_T^{-1} \) to the new domain is shown by \( \overrightarrow{WD_T} \), this matrix has a structure similar to \( \overrightarrow{WD} \) :

\[ \overrightarrow{WD_T} = \begin{pmatrix} \overrightarrow{HH} & \overrightarrow{HL} \\ \overrightarrow{LH} & \overrightarrow{LL} \end{pmatrix} \]  
(34)

To compute \( i^{th} \) value of \( \overrightarrow{HH}, \overrightarrow{HL}, \overrightarrow{LH}, \overrightarrow{LL} \) this relation is used:

\[ \begin{pmatrix} hh_i' \\ hl_i' \\ lh_i' \\ ll_i' \end{pmatrix} = \begin{pmatrix} hh_i \\ hl_i \\ lh_i \\ ll_i \end{pmatrix}^{-1} \]  
(35)

where \( hh_i, hl_i, lh_i \) and \( ll_i \) are the \( i^{th} \) values of \( \overrightarrow{HH}, \overrightarrow{HL}, \overrightarrow{LH}, \overrightarrow{LL} \) .

3.1.4. Transmission Line

Writing relations of voltage and current drop for a differential part of transmission line leads to:

\[ -\frac{\partial v}{\partial x} = ri + l \frac{\partial i}{\partial t} \]  
(36)

\[ -\frac{\partial i}{\partial x} = g_v + c \frac{\partial v}{\partial t} \]  
(37)

If (36) replaced in (37), then we have:

\[ -\frac{\partial^2 v}{\partial x^2} = r_i v + r_i \frac{\partial v}{\partial t} + r_i \frac{\partial^2 v}{\partial t^2} \]  
(38)

Where:

\[ r_i = r \cdot g, \quad r_i = r_i \cdot c + 1 \cdot g, \quad r_i = l \cdot c \]

if (38) is transformed to the new domain for \( i^{th} \) element of \( j^{th} \) level, one can gets:

\[ \begin{pmatrix} \frac{\partial V_{i,j}}{\partial x} \\ \frac{\partial V_{i,j}}{\partial t} \end{pmatrix} = \begin{pmatrix} r_i + r_i hh_i' + r_i hl_i' \\ r_i lh_i' + r_i ll_i' \end{pmatrix} \begin{pmatrix} V_{i,j} \\ V_{i,j} \end{pmatrix} \]  
(39)

Where \( hh_i', lh_i', hl_i', ll_i' \) are the \( i^{th} \) diagonal elements of \( \overrightarrow{HH}, \overrightarrow{HL}, \overrightarrow{LH}, \overrightarrow{LL} \) and \( \overrightarrow{HH}, \overrightarrow{HL}, \overrightarrow{LH}, \overrightarrow{LL} \) respectively where:

\[ HH^2 = H \cdot D_T^2 \cdot H^2, \overrightarrow{HL}, \overrightarrow{LH}, \overrightarrow{LL}^2 = L \cdot D_T^2 \cdot L^2 \]  
(40)

And \( D_T^2 \) is the discretized form of second order derivative operator.

As shown in fig.1, adjusting of parameters for a frequency dependent transmission line can be done comfortably.

This approach of modeling can be used for three phase transmission lines using a modal matrix to separate the wave equation of each phase to another. It can be shown the operation of the modal matrix in the new domain is same as time domain.

3.1.5. Switching Devices Modeling

In this part the modeling method for switching devices is investigated briefly. Modeling of these devices is explained by many of researchers for harmonic studies \[27]-[31]. Assume that a linear load is connected to network in series with a power electronic switch. The relation between voltage and current of load without considering switch is:

\[ v(t) = f(v(t)) \]  
(41)

Where in (77), \( f \) is a linear operator. As the load is in series with the switch, the relation between current and voltage ofswitching load is:

\[ i(t) = p(t) \cdot f(p(t) \cdot v(t)) \]  
(42)

Where \( p(t) \) is switching signal. Switching signal is a periodic function. Disceretizing of equation (42) leads to:

\[ L = [S] \cdot V \]  
(43)

Where:
\[ [S] = [P] \cdot [F] \cdot [P] \quad (44) \]

It is not necessary to suppose that the switching device is synchronized with power system frequency. Transferring (44) to the new suggested domain doesn’t result a diagonal matrix. This refers to existence of cross-couplings between harmonics. As the transferred matrix is not diagonal, so using of this matrix in network equation directly makes difficulties in numerical solution. To avoid from this problem, this matrix is not considered in admittance matrix directly and the solution is obtained in a repetitive procedure.

3.2. Network Representation

To develop this method for power network simulation, a simple circuit is considered (Fig. 2). Writing the KCL relation leads to:

\[ -i_s + \frac{v_m}{r} + c \frac{d}{dt}v_m + \frac{1}{r} \int v_m dt = 0 \quad (45) \]

According to the modified nodal method that is used in harmonic analysis:

\[ \begin{bmatrix} 1 + \frac{cp}{1} & \frac{1}{p} & 1 \\ \frac{1}{r} \\ 0 \end{bmatrix} \begin{bmatrix} v_1 \\ v_m \\ i_s \end{bmatrix} = \begin{bmatrix} 0 \\ 0 \end{bmatrix} \quad (46) \]

Where \( p \) is derivative operator.

Now (37) is disceretized as follows:

\[ \begin{bmatrix} \frac{1}{r} U + c \cdot D_r + \frac{1}{r} D_r^{-1} \quad U \\ U \quad 0 \end{bmatrix} \begin{bmatrix} v_1 \\ I_s \end{bmatrix} = \begin{bmatrix} 0 \\ v_m \end{bmatrix} \quad (47) \]

where \( U \) is a unit matrix, response and input vectors are shown in capital letters. If (47) is transformed to MRA space and then diagonal sub-matrices are obtained using (19) and (20) (or mapping (47) to the new domain), the results would be as follows:

- \( a_{n,i} = \begin{bmatrix} \frac{1}{r} + c \cdot hh' + \frac{1}{r} \quad hh' \\ 1 \\ 0 \end{bmatrix} \quad (54) \)
- \( b_{n,i} = \begin{bmatrix} c \cdot hl + \frac{1}{r} \quad hl' \\ 0 \\ 0 \end{bmatrix} \quad (55) \)
- \( c_{n,i} = \begin{bmatrix} c \cdot hl' + \frac{1}{r} \quad hl'' \\ 0 \\ 0 \end{bmatrix} \quad (56) \)
- \( t_{n,i} = \begin{bmatrix} \frac{1}{r} + c \cdot ll + \frac{1}{r} \quad ll' \\ 1 \\ 0 \end{bmatrix} \quad (57) \)

(38) can be written as follow:

\[ \begin{bmatrix} C_R + pC_L + \frac{1}{p} C_L \\ 1 \\ 0 \end{bmatrix} \begin{bmatrix} x_s \\ i_s \end{bmatrix} = \begin{bmatrix} 0 \\ v_m \end{bmatrix} \quad (58) \]

where:

\[ C_R = \begin{bmatrix} \frac{1}{r} \\ 1 \\ 0 \end{bmatrix}, \quad C_L = \begin{bmatrix} 0 \\ 1 \\ 0 \end{bmatrix}, \quad C_L = \begin{bmatrix} 0 \\ 0 \\ 0 \end{bmatrix} \quad (59) \]
$C_R$, $C_C$ and $C_L$ are respectively resistive coefficients matrix, capacitive coefficients matrix and inductive coefficients matrix. These matrices can be defined according to the modified nodal method. By applying (58) and (59), (54) to (57) are rearranged as follow:

\[ a_{i,j} = C_R + h h_i \cdot C_C + h h'_i \cdot C_L \]  
\[ b_{i,j} = h h_i \cdot C_C + h h'_i \cdot C_L \]  
\[ c_{i,j} = l h_i \cdot C_C + l h'_i \cdot C_L \]  
\[ t_{i,j} = C_R + l l_i \cdot C_C + l l'_i \cdot C_L \]

The formulas (60) to (63) are written for any network directly. Now using these matrices the $i^{th}$ value of response vectors are computed:

\[ r_{i,j} = t_{i,j} \left[ a_{i,j}^{-1} b_{i,j} \right] \]  
\[ s_{i,j} = r_{i,j}^{-1} \left( s_{i,j} - c_{i,j} a_{i,j}^{-1} d_{i,j} \right) \]  
\[ d_{i,j} = a_{i,j}^{-1} \left( d_{i,j} - b_{i,j} s_{i,j} \right) \]

To obtain $j^{th}$ level of response vector in MRA space, i.e. $d_{i,j}$ and $d_{i,j}'$, $\Gamma$ is multiplied to $\hat{d}_{i,j}$ and $\hat{s}_{i,j}$ respectively.

The steps for Nonsinusoidal steady state analysis are as follow:
1. Determine number of levels ($J_{\max}$) and number of samples (N). $J_{\max}$ is the index of finest scale in multiresolution space.
2. Calculate the $C_R$, $C_C$ and $C_L$ matrices according to modified nodal method.
4. Set $j=J_{\max}-J$. $J$ is the index of current resolution level.
5. Compute $D_T$ for $j^{th}$ level.
6. Compute the $\Gamma$ matrix using (20) and then transfer the input vector to the new domain.
7. Set $i=1$.
8. Calculate $a_{i,j}$, $b_{i,j}$, $c_{i,j}$ and $t_{i,j}$ using (60) to (63). Then using (64) - (66) calculate $\hat{d}_{i,j}$ and $\hat{s}_{i,j}$.
9. If $i$ is equal to N/2 then set $i=i+1$ and goto step 8.
10. Calculate the response vector in MRA space for $j^{th}$ resolution level, (i.e. $d_{i,j}$ and $s_{i,j}$).
11. If $J$ is not equal to $J_{\max}$ set $J=J+1$ and go to step 5.
12. End.

Fig. 3 shows the flowchart of nonsinusoidal steady state analysis in the proposed domain.

4. Case Study 1
In this section, the proposed method is demonstrated for a case study that is a test system for harmonic simulation [26]. Fig. 4 shows a single line diagram of this network, a harmonic source where is located on the bus 49-RECT. For lines and transformers a simple model is used and the frequency dependency is neglected. The test system is connected to a larger plant from 100: Util-69 bus. So for the larger plant an equivalent is obtained from the fault MVA level.
suggested domain and the values of THDs are computed directly from results in this domain. The consumed time for simulation of test network was found to be 4.7 sec. Simulation, which was coded with MATLAB ver. 7, was carried out in this work using 512 samples, 3 levels for MRA space and using a personal computer with Pentium 4 CPU (2.8GHz) and 512RAM. To compare this approach with the time domain method, the currents of both the local generator and the utility plant are plotted in Fig. 5 and Fig. 6 respectively. In table I and II, some of the computed THDs are compared with those obtained from SIMULINK model using FFT.

### Table 1: THD Percentage Values

<table>
<thead>
<tr>
<th>Bus Voltages</th>
<th>New proposed method</th>
<th>Time domain method</th>
<th>Error (%)</th>
</tr>
</thead>
<tbody>
<tr>
<td>49-RECT</td>
<td>2.48</td>
<td>2.57</td>
<td>3.568</td>
</tr>
<tr>
<td>05:FDR F</td>
<td>2.41</td>
<td>2.52</td>
<td>4.400</td>
</tr>
<tr>
<td>09:FDR H</td>
<td>2.40</td>
<td>2.52</td>
<td>4.789</td>
</tr>
<tr>
<td>03: MILL</td>
<td>2.41</td>
<td>2.52</td>
<td>4.396</td>
</tr>
<tr>
<td>50:GEN-1</td>
<td>2.32</td>
<td>2.43</td>
<td>4.497</td>
</tr>
<tr>
<td>100:UTIL-69</td>
<td>0.17</td>
<td>0.18</td>
<td>3.111</td>
</tr>
</tbody>
</table>

### Table 2: THD Percentage Val UES

<table>
<thead>
<tr>
<th>Current</th>
<th>New proposed method</th>
<th>Time domain method</th>
<th>Error (%)</th>
</tr>
</thead>
<tbody>
<tr>
<td>I_{U1}</td>
<td>2.49</td>
<td>2.54</td>
<td>2.106</td>
</tr>
<tr>
<td>I_{G1}</td>
<td>20.54</td>
<td>21.16</td>
<td>2.945</td>
</tr>
</tbody>
</table>

5. Case Study 2

To examine the validation of introduced models for distributed transmission line and switching devices a 132 KV single phase test system is selected and simulated via the new suggested domain. This simple system consists of three transmission lines and a switching load (Fig. 7). The switching load is a half bridge thyristor rectifier and it is supposed the firing angle is 5°. In table III test system parameters are presented. In Fig. 8 and Fig. 9 the results from time domain and new suggested domain simulations are compared. Also in table IV the THD percentages and the consumed times for this simulation are compared. The THDs are calculated directly from the new proposed domain simulation results with out transferring them to time domain. In this simulation db4 wavelet function is used and the time domain simulation is done with MATLAB software. It must be noted that none of fast numerical methods such as spares matrix methods are
employed. However using fast numerical algorithms, especially in transferring input vectors and operators to the new domain, decrease the simulation time significantly.

**Fig. 7: Test system.**

![Test system diagram](image)

**Fig. 8: Switching load current, line: New proposed domain; dash-line: Time domain.**

![Switching load current graph](image)

**Fig. 9: \( V_3 \), line: New proposed domain; dash-line: Time domain.**

![Voltage graph](image)

5. Conclusion

In this paper a new algorithm for power system study and simulation in nonsinusoidal and periodic conditions via a new domain is introduced. The algorithm was applied to simulation of a relevant large test system containing a harmonic source. To show the ability of this domain for practical aims a single phase system with distributed transmission lines and a switching load was simulated. The model of switching device was based on switching signal. In such simulation the interaction between network and switching device was considered. The capabilities of this new method via new space make it possible to develop new applications in several fields such as power quality.

6. References


